An evaluation of a new type of High Efficiency Hybrid Gate Drive Circuit for SiC- MOSFET suitable for Automotive Power Electronics System Applications

Masayoshi Yamamoto†, member and Shinya Shirai††, non member, Senanayake Thilak‡, non-member and Jun Imaoka†, member and Ryosuke Ishido+++ , non-member and Yuta Okawauchi+++ , non-member and Ken Nakahara+++ , non-member

SUMMARY In response to fast charging systems, Silicon Carbide (SiC) power semiconductor devices are of great interest of the automotive power electronics applications as the next generation of fast charging systems require high voltage batteries. For high voltage battery EVs (Electric Vehicles) over 800V, SiC power semiconductor devices are suitable for 3-phase inverters, battery chargers, and isolated DC-DC converters due to their high voltage rating and high efficiency performance. However, SiC-MOSFETs have two characteristics that interfere with high-speed switching and high efficiency performance operations for SiC MOSFET applications in automotive power electronics systems. One characteristic is the low voltage rating of the gate-source terminal, and the other is the large internal gate-resistance of SiC MOSFET. The purpose of this work was to evaluate a proposed hybrid gate drive circuit that could ignore the internal gate-resistance and maintain the gate-source terminal stability of the SiC-MOSFET applications. It has been found that the proposed hybrid gate drive circuit can achieve faster and lower loss switching performance than conventional gate drive circuits by using the current source gate drive characteristics. In addition, the proposed gate drive circuit can use the voltage source gate drive characteristics to protect the gate-source terminals despite the low voltage rating of the SiC MOS-FET gate-source terminals.

key words: SiC-MOSFET, Gate-driver, Current-source, Voltage-source. Gate resistance

1. Introduction

Electric Vehicle (EV) technical trend have been attracted great interest from all over the world because of its growing great market until 2030. Figure 1 shows each automotive company’s sales quantity compared between 2019 and 2020. In spite of COVID-19 calamity, it is understood that only TESLA have expanded their sales as in Fig.1. The reason is long cruising range for one full charging condition in TESLA EV products. In general, the long cruising range performance is decided from total balance between the coefficient of drag (CD) value and heavy weight of EV. Model 3 and Model S of TESLA EV can achieve higher balance performance in each component as compared with Taycan / Porsche as in Fig.2. From this discussion, it can be seen that the most important performance for automotive applications is high power density performance [1].

In addition, compared to traditional technologies, next-generation EV applications require additional technology to achieve high power density performance.

The electric system for EV is composed of the on-board charger, the isolated DC-DC converter, main drive inverter and traction motor in general. And each electric components will mount and laminated as shown in Fig. 3. In this case, each electric components must keep low profile performance because the higher automobile hoods influence directly for CD value of EVs.

To achieve the low-profile performance, several technical challenges will be required in next generation EV applications as shown in Fig. 4. Mainly, the necessary
Fig. 4 Technical requirement for low profile performance of EV system

Fig. 5 Power Electronics System for EV (Jaguar I-Pace, 2020)

technical components can be divided into two parts, which is a high frequency and a high efficiency technology. In case of high frequency condition, passive components will be achieve high power density and miniaturized performance [2]-[5]. And high frequency system requires higher performance control method in both of analogue and digital feedback systems [6]-[14]. However, high frequency system includes noise problem in DC bus-line for EV. In electric system for EV, there are many numbers of DC-DC converters connected in parallel to DC bus-line, therefore, each DC-DC converter EMI/EMC noise control requires effective measures [15]-[19]. This is because if noise appears on the DC bus line, it will affect the end application of each DC-DC converter over the DC bus line.

The DC bus-line application such as auxiliary battery charger in HEV/EV, is important too and as a solution of preventing noise, isolated DC-DC converter, its combination systems and DC breaker have been reported in recent years [20]-[36].

On the other hand, high efficiency technique contributes to miniaturized cooling systems of power electronics system for EV. Because power electronics components related to power losses is account for half volume of power electronics systems for EV as shown in Fig. 5. Therefore, the reduction of power losses in Power Electronics systems is effective solution for high power density technical hurdle.

Most effective solution to the technical hurdles of high power density is to replace power devices with next generation power semiconductor devices such as Silicon Carbide(SiC), Gallium Nitride(GaN) and Gallium Oxide [37]-[39] due to their high-performance characteristics of low device power loss. However, the cost problem remains for such power device applications. In addition, soft switching techniques can effectively reduce power losses in power electronics systems with traditional silicon devices. On the other hand, soft switching techniques require additional circuitry and control systems for perfect zero voltage switching (ZVS) and zero current switching (ZCS) in switching transient of each power semiconductor devices [40]-[47]. Therefore, using soft switching technology increases cost and space. Replacing silicon devices with SiC makes GaN a reasonable solution and at a relatively low cost.

In this paper, the combination solution has been selected for high power density performance for power electronics system. That is combination technique between SiC power semiconductor device applications and its gate drive circuit development. Because SiC power device have been already applied in Electric Vehicle, Model 3/TESLA [48]. However, the conventional gate drive circuit has been applied in such EV, but improved gate drive circuit can reduce power losses as compared with conventional gate drive circuit. Our effort is to propose novel gate driver circuit to mitigate the gate driving problem and reduce the power losses.

2. Characteristics of SiC MOSFET and Gate-driving problems

SiC-MOSFETs, which are next-generation power semiconductors, have greater advantages over conventional silicon MOSFETs and IGBTs in high voltage switching power supply applications. However, in consideration of the characteristics of SiC-MOSFET from the point of view of the gate drive, it can be seen that the characteristics of SiC-MOSFET have several problems [49]-[50].

One of the main points is that the internal gate resistance RG
(int) is large as compared with the same specification (device voltage) of silicon MOSFET. Fig.6 is a diagram in which more than 1000 MOSFETs are examined and among them, those in which the internal gate resistance and the input capacitance are described in the data sheet are extracted and the time constant is plotted.

As seen from Fig.6, the SiC-MOSFET has a large time constant. Compared to silicon MOSFETs, SiC-MOSFETs can achieve lower on-resistance on smaller area chips, reducing gate input capacitance. However, currently, polysilicon is mainly used as the gate electrode material for SiC-MOSFETs fabrication process to get high switching speed, but it has higher resistance and higher gate resistance than the silicide used for silicon MOSFETs. In addition, for modular products consisting of multiple Si or SiC chips, gate waveform disturbance is common and has an undesired effect on switching transients. A damping resistor is inserted in each chip to suppress the disturbance of the waveform. However, the internal gate resistance of SiC is higher than that of Si, and the gate resistance of SiC increases with the damping resistance.

Therefore, the time constant of the internal gate resistance is several times that of the silicon MOSFET, and there is a problem that high-speed driving is difficult with a general voltage source type gate drive circuit.

The second point is that the gate withstand voltage is low. In the case of a voltage source type gate drive circuit, there is a way to increase the gate drive voltage in order to overcome the deceleration of the gate drive due to the internal gate resistance. However, since the difference between the rated drive voltage of the gate and the absolute maximum rated voltage of the SiC-MOSFET is small, if the gate drive voltage is easily increased, there is a risk of withstand voltage failure due to ringing. The current source type gate drive circuit can drive the gate at high speed without being affected by the internal gate resistance, but in the case of the driver circuit in Fig.7, there is an inductor and the gate input capacitance of the SiC-MOSFET. Therefore, the steady-state gate voltage may not be as designed and the gate withstand voltage may be exceeded.

Third point, the transconductance is small, and the ON resistance fluctuates greatly due to fluctuations in the gate voltage. In this respect, a voltage source type gate drive circuit in which the gate drive voltage in a steady state is stable is advantageous. In the current source type gate drive circuit, as in Fig.7, the gate drive voltage in the steady state gradually decreases due to the gate leak current. Therefore, there is a risk that the loss will increase due to the increase in ON resistance. In addition, due to the low transconductance of SiC-MOSFETs, the ON resistance has a negative coefficient with respect to temperature in the low gate voltage range. Therefore, in a drive circuit such as a current source type gate drive circuit in which the gate drive voltage drops during steady operation, the SiC-MOSFET may risk of thermal runaway.

3. Proposed hybrid gate driver System

In the previous section, we explained the problems when using a conventional gate drive circuit for the gate drive of SiC-MOSFET. Therefore, we realized that driving a SiC-MOSFET needs gate driver circuit that allows current to flow through the gate regardless of the internal gate resistance, and the characteristics of a voltage source-type gate drive circuit that stabilizes the gate voltage during steady state operation. Therefore, in this paper, we propose a new gate drive circuit that realizes high-speed and stable gate drive by charging the gate at high-speed using an inductor that acts as a current source at the time of rising and falling, and then shifting to voltage source type drive in order to realize the optimum gate drive of SiC-MOSFET.

3.1 Configuration of proposed gate driver circuit

The proposed circuit configuration is shown in Fig.8. The area surrounded by the gray dotted line on the left side is the proposed gate drive circuit, and the QM is the targeted SiC-MOSFET. The proposed circuit consists of four switching elements (Q1a, Q1b, Q2, Q3), two diodes (D1, D2), power supplies (E1, E2) with voltage V/2, and an inductor (L). The gate voltages of Q1a, Q1b, Q2, and Q3 are set to VGS(Q1a), VGS

![Proposed Gate Driver Circuit](image)

Fig.7 Current source type gate driver circuit

Fig.8 Proposed hybrid gate driver circuit

Fig.9 Gate control signal distribution circuit
Let the gate voltage seen from above be \( v_{GS(\text{ext})} \) and the gate oxide film voltage be \( v_{GS(\text{int})} \). The gate voltage when \( Q_M \) is on is \( V_G \), which is the rated gate voltage or recommended gate drive voltage described in the data sheet of the SiC-MOSFET used.

3.2 Operating principle

As shown in Fig. 9, the gate control signal of each switching element that composes the proposed gate driver circuit is generated from the PWM command from the external controller. In the proposed circuit, each MOSFET has a simple operation of turning on and off only once per cycle of the input PWM signal, so it can be operated with such a simple distribution circuit. In an actual circuit, if \( Q_2 \) and \( Q_3 \) are turned on at the same time, a shoot-through current will flow, so it is necessary to set a dead time at each switching. For \( Q_{1b} \) and \( Q_{1b} \), dead time is not required because the switching is performed when the current of the inductors connected in series is zero. Fig.10 shows the key waveforms and operating modes of the proposed gate drive circuit.

3.3 Operating modes of proposed circuit

Fig.11 shows the operating modes of proposed gate driver circuit and each mode of circuit operation is explained in section 3.3

<Mode 1> As shown in Fig.11(a), \( Q_{lb} \) and \( Q_3 \) are in the ON state, and \( Q_{la} \) and \( Q_2 \) are in the OFF state. This mode is the preparation period for turning on the SiC-MOSFET to be driven. Current flows from the power supply \( E_2 \) as shown by the gray solid arrow in Fig.11(a), and the inductor \( L \) is excited. At the time of \( T_1 \), \( Q_2 \) is turned on and \( Q_3 \) is turned off to move to the next mode. Since the current \( i_L \) of the inductor \( L \) increases linearly, if the exciting time is \( t_{ex} = T_1 - T_0 = T_2 - T_3 \) and the forward voltage of the body diode of \( Q_{la} \) and \( D_2 \) is \( V_f \), the value of \( i_L \) at \( T_1 \) is given by (1). Although \( V_f \) is current-dependent, its fluctuation is very smaller than the voltage \( V_G / 2 \) of the power supply \( E_2 \) and it can be ignored.

\[
i_L(T_1) = \frac{V_G}{2} - 2V_f \leq \frac{t_{ex}}{L} \leq \frac{V_G}{2}
\]

<Mode 2> As shown in Fig.11(b), \( Q_{lb} \) and \( Q_2 \) are in the ON state, and \( Q_{la} \) and \( Q_3 \) are in the OFF state. The SiC-MOSFET turns on when the current of the inductor \( L \) excited in Mode 1 passes through the gate of the SiC-MOSFET to be driven. At this time, the inductor \( L \) behaves as a current source, so...
the gate current is not limited to the internal parasitic gate resistance $R_{G\,(int)}$ of the SiC-MOSFET. In other words, it is a current source type drive, and high-speed gate drive is realized.

<Mode 3> As shown in Fig.11(c), after the gate of the SiC-MOSFET is fully charged by the action of the inductor $L$, the gate of the SiC-MOSFET is clamped to $V_g$ by $Q_2$ turned on in Mode 2, and the voltage stabilizes. This mode is voltage source type drive. The transition from Mode 2 to Mode 3 is performed at $T_6$, but at this time, no command from the external controller is required, and the transition occurs naturally when the current of the inductor $L$ becomes zero.

<Mode 4> As shown in Fig.11(d), $Q_{Ib}$ and $Q_2$ are in the ON state, and $Q_{Ob}$ and $Q_2$ are in the OFF state. This mode is equivalent to Mode 1 except that the direction of the current is opposite, and it is the preparation period for turning off the SiC-MOSFET to be driven. A current flow from the power supply $E_I$ as shown by the gray solid arrow in Fig.11(d), and the inductor $L$ is excited. At the time of $T_6$, $Q_2$ is turned on and $Q_3$ is turned off to move to the next mode.

<Mode 5> As shown in Fig.11(e), $Q_{Ib}$ and $Q_2$ are in the ON state, and $Q_{Ob}$ and $Q_2$ are in the OFF state. The SiC-MOSFET turns off when the gate charge of the SiC-MOSFET to be driven is pulled out at once by the inductor $L$ excited in Mode 4. At this time, the inductor $L$ behaves as a current source, so the gate current is not limited to the internal parasitic gate resistance $R_{G\,(int)}$ of the SiC-MOSFET. In other words, it is a current source type drive, and high-speed gate drive is realized.

<Mode 6> As shown in Fig.11(f), after the gate of the SiC-MOSFET is fully charged by the action of the inductor $L$, the gate of the SiC-MOSFET is clamped to 0V by $Q_2$ turned on in Mode 5, and the voltage stabilizes. This mode is voltage source type drive. The transition from Mode 5 to Mode 6 is performed at $T_7$, but at this time, no command from the external controller is required, and the transition occurs naturally when the current of the inductor $L$ becomes zero.

### 4. Design of hybrid gate driver circuit

When driving a MOSFET, it is necessary to design the gate drive circuit so that the gate oxide film voltage does not exceed the absolute maximum rated voltage, but the inductor $L$ that operates as a current source in the proposed circuit also has a large constant and is driven. The gate-source voltage of the target SiC-MOSFET exceeds the absolute maximum rating value, which may cause a malfunction. Conversely, if the inductor constant is too small, the inductor will give less energy to the gate drive of the driving SiC-MOSFET, making it impossible to speed up the gate drive. Therefore, in the proposed circuit, it is important to properly determine the constant of the inductor $L$ that operates as a current source. However, since it is difficult to directly measure the voltage of the gate oxide film, it is necessary to estimate the voltage of the gate oxide film by calculation at both the design stage and the actual machine verification stage. Therefore, focusing on the amount of charge flowing through the gate of the SiC-MOSFET driven from the inductor $L$, the gate oxide film is based on the relationship of the gate charge amount $(Q_g=\int I_g(t)\,dt)$ and gate voltage $(V_{gs})$.

ROHM's switching device BSM300D12P2E001[51] is selected as the SiC-MOSFET to be driven in our design. The absolute maximum rating of the SiC-MOSFET is shown in Table 1, and the actual measurement graphs of $Q_g$ and $V_{gs}$ are shown in Fig.12. As can be read from this graph, $Q_g$ and $V_{gs}$ show a non-linear relationship. In particular, since the feedback capacitance is charged in the mirror plateau region, the slope of the $Q_g-V_{gs}$ graph becomes zero. Here, the

![Fig.12 Actual measurement of Qg–Vgs of SiC-MOSFET (BSM300D12P2E001)](image)

Fig.13 Simplified circuit of the proposed gate driver in different regions of gate charge

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Symbol</th>
<th>Limit</th>
</tr>
</thead>
<tbody>
<tr>
<td>Drain-source voltage [V]</td>
<td>$V_{DSS}$</td>
<td>1200</td>
</tr>
<tr>
<td>Gate-source voltage [V]</td>
<td>$V_{GGS}$</td>
<td>-6 to 22</td>
</tr>
<tr>
<td>Drain current [A]</td>
<td>$I_D$</td>
<td>300</td>
</tr>
<tr>
<td>Source current [A]</td>
<td>$I_S$</td>
<td>300</td>
</tr>
</tbody>
</table>
analysis is carried out by dividing into three areas as shown in Fig. 12. However, in the proposed circuit, the current drive is performed until the end of the mirror plateau region, so only Region 1 and Region 2 are designed so that the inductor current contributes to the gate drive. Therefore, the regions to be analyzed are only Region 1 and Region 2, and the inductor value and excitation time can be determined by calculating the gate current in this region. As a simpler design method, there is a method of designing using a circuit simulator. The value of the inductor L and the excitation time should be adjusted so that the gate drive current flows through the SiC-MOSFET to be driven even after the current of the inductor L of the proposed gate drive circuit becomes zero. On the contrary, if a current flows from the inductor to the gate of the SiC-MOSFET even after reaching the target gate drive voltage, not only the gate withstand voltage is exceeded, but also the voltage source type drive cannot be shifted, resulting in unstable operation.

<Region 1> As shown in Fig. 12, in region 1, the proposed circuit can be simplified as in Fig. 13(a), and gate current can be expressed as (2)

\[ L \frac{di_G(t)}{dt} + R_{G(int)}i_G(t) + \frac{1}{C_{iss}} \int i_G(t)dt = \frac{V_G}{2} \]  

After number of calculation step gate current \(i_G\) in region 1 can be derived as (3)

\[ i_G(t) = I_0ae^{-\frac{R_{G(int)}}{2L}t} \sin(\omega t + \varphi) \]

where

\[ a = \sqrt{1 + \left(\frac{R_G - R_{G(port)}}{2mL_0}\right)^2}, \quad \omega = \frac{1}{\sqrt{L_{iss}} - \frac{R_{G(port)}}{L}}, \quad \varphi = \tan^{-1}\left(\frac{2mL_0}{V_G - R_{G(port)}L}\right) \]

<Region 2> As shown in Fig. 12, region 2 is the mirror plateau region, and since the charge flows from the drain side to the gate side via the feedback capacitance, the slope of the \(Q_g-V_{gs}\) graph becomes zero. That is, the gate and source of the SiC-MOSFET to be driven behave as a constant voltage source of \(V_{gs(plateau)}\). Therefore, the proposed circuit can be simplified as shown in Fig. 13(b). If the inductor current entering this region, is \(I_L\), the gate current can be expressed as (4)

\[ i_G(t) = \frac{V_G}{2R_{G(int)}} + \left(I_L - \frac{V_G}{2R_{G(int)}}\right)e^{-\frac{R_{G(int)}}{L}t} \]  

5. Simulation

The operation of the proposed gate driver circuit was confirmed by the circuit simulator. The circuit simulator used is LTspice provided by Analog Devices, Inc. The simulation circuit is shown in Fig. 14. In the studies so far, the gate drive voltage of the SiC-MOSFET was 0V when it was off, but in actual applications, the gate drive voltage when it is off is often set to a negative voltage in order to avoid malfunctions. Therefore, in simulations and experiments, a 2V constant voltage source was inserted between the Kelvin source terminal of the SiC-MOSFET and the proposed gate drive circuit, and the VG was set to 20V so that the drive could be from -2V to 18V bottom. The gate drive voltage only shifts as a whole, and the operation...
6. Experimental verification

Experimentally driven the SiC-MOSFET using the proposed gate drive circuit and verified the effect of increasing the switching speed in the double pulse test circuit.

<table>
<thead>
<tr>
<th>(a)</th>
<th>Voltage measurement</th>
<th>(b)</th>
<th>Current measurement</th>
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<tbody>
<tr>
<td>(c)</td>
<td>Points of voltage and current measurement of experimental prototype. Current measured between MLCC array and drain-source.</td>
<td></td>
<td></td>
</tr>
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</table>

6.1 Method and techniques of measurements

Fig.17 shows the experimental setup with the enlarged view. Using the Tektronix DPO5204B oscilloscope (frequency band 2 GHz, sampling rate 10GS/s), waveform of the experimental prototype was measured.

In the double pulse test, various measures are required to measure a waveform that is closer to the true waveform. Especially in the case of high-speed switching devices such as SiC-MOSFETs, the waveform becomes violent due to the parasitic inductance of the circuit. In the case of the SiC-MOSFET module used this time, the parasitic inductance inside the package is large, so it is important to reduce the parasitic inductance of the external circuit.

Fig.18(a) shows the measurement points of the drain-source voltage waveform. A wideband passive probe (Tektronix P5100A) was used to measure the drain-source voltage waveform. Although different passive probes are connected in Fig.18(a), P5100A was used in the waveform measurement. The waveform measured from the chip of the passive probe to the drain source of the switching device and the inductance of the ground lead of the passive probe is greatly affected. In addition, due to the wiring inductance inside the module, when measurement is performed at the terminal where a large current flows, a waveform that is significantly different from the waveform of the internal SiC-MOSFET chip is observed. Therefore, in the experimental verification, the substrate was placed directly above the SiC-MOSFET module, the passive probe was fixed without using a ground lead as shown in Fig.18(a), and measurement was performed between the sensing drain terminal and the Kelvin source.

![Image](image_url)

Fig.19 Experiment results for comparison of switching waveforms of conventional and proposed topologies at 200V/50A

![Image](image_url)

Fig.20 Gate current and gate charge $Q_G - V_{GS}$ with proposed gate driver when driving a SiC-MOSFET
Furthermore, as in Fig.18(b), the MLCC (Multilayer Ceramic Capacitor) connected between the PN terminals of the MOSFET and the current probe used to measure the drain-source current. A low-impedance MLCC was placed in the immediate vicinity between the PN terminals of the MOSFET, and the current measurement loop was also devised to minimize the ringing of the waveform.

6.2 Experimental results

Measured results of the proposed gate driver circuit using the experimental prototype will be described. Fig.19 shows the waveform of the test results with a drain-source voltage of 200V and a drain-current of 50A. In both Fig.19(a) and Fig.19(b), the solid line is the waveform when the SiCMOSFET module is driven using the proposed gate drive circuit, and the broken line is the waveform when the conventional voltage source type gate drive circuit is used. The blue line is the drain-source voltage waveform, and the red line is the drain-source current waveform. Furthermore, Fig.19(c) and Fig.19(d) show the losses at turn-on and turn-off, respectively. The red area is the loss when the proposed gate drive circuit is measured, and the black area is the loss when the conventional voltage source type gate drive circuit is measured. Similar to the simulation study, it was confirmed that the switching speed was increased for both turn-on and turn-off. When the switching loss was calculated, the turn-on loss shown in Fig.19(c) was 359 μJ for the conventional voltage source type gate drive circuit and 203 μJ when the proposed gate drive circuit was used. 43.5% of turn-on loss reduction is achieved with proposed gate driver circuit. Similarly, regarding the loss at turn-off, 27.7% loss reduction is achieved. 141 μJ when using the conventional voltage source type gate drive circuit and 102 μJ when using the proposed circuit.

Fig.20 shows the measurement results of the gate current at turn-on switching when the SiC-MOSFET is driven with proposed gate driver circuit. When the gate current waveform was integrated, the amount of charge that flowed was 1300 nC. When the gate oxide film voltage is read from Fig.20(b), it is found to be 18V. Therefore, it was confirmed that the current drive was shifted to the voltage drive as designed in the middle of the gate drive, and that safe drive was possible without exceeding the gate withstand voltage.

7. Conclusions

In this paper, we have explained the problems from the viewpoint of gate drive of SiC-MOSFET as compared with silicon MOSFET. High internal gate resistance and low transconductance can slow down switching speeds and fluctuate gate drive voltages, which can lead to high SiC-MOSFET losses. In addition, since the margin of the gate withstand voltage is smaller than the recommended gate drive voltage, the method of increasing the gate drive voltage for high-speed switching cannot be adopted, and stable gate drive is required. Therefore, in order to mitigate the above gate drive problem, a hybrid gate driver is proposed, confirmed by Lt-spice simulation, and experimentally verified. Significant results were achieved with a 43.5% reduction in turn-on switching loss and a 27.7% reduction in turn-off switching loss.

References

[16] H. Hasegawa, K. Harada, Y. Ishihara, and T. Todaka, ”An
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Discussion of SiC/GaN Power Semiconductor

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Resonant Voltage

Commun., Vol. E95

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Masayoshi Yamamoto (Member) received his M.S. and Ph.D. degree in science and engineering from Yamaguchi University, Yamaguchi, Japan in 2000 and 2004 respectively. From 2004 to 2005, he was with Sanken Electric Co., Ltd., Saitama, Japan. From 2006 to 2017, he was with the Interdisciplinary Faculty of Science and Engineering in Shimane University, Japan, as an Associate Professor. He is currently a Professor at Institute of Materials and Systems for Sustainability (IMaSS), Nagoya University, Japan. His research interests include power supply for HEV (boost converter, buck converter, 3-phase inverter, digital control), charging system for EV, LED illumination system for a tunnel, EMI of switching power supply, and wireless power transfer.

Shinya Shirai (Non-member) received his B.S. and M.S. degrees in Electrical Engineering from Nagoya University, Nagoya, Japan in 2019 and 2021, respectively. He had studied gate drive circuits for wide bandgap power semiconductors and ultra-high voltage isolated gate driver for HVDCs. Since 2021 he has been with Mitsubishi Heavy Industries, Ltd.

Senanayake, Thilak (non-member) received the B.S degree from University of Colombo, Sri Lanka, in 1991, M.E., and Ph.D degrees in Electronics Engineering from the Kyushu University, Japan, in 2001,2004, respectively. From 2005-2010 and 2010-2015 he was a Research Scientist in Toyota Central Research and Development Laboratory Inc., and DENSO Corporation, Japan respectively, where he was involved with research and development of low cost, high reliable, and miniaturization of power control unit of the Hybrid /Electric vehicles. From 2015-2019, he was a Research Scientist with Power Electronics Laboratory, University of Tsukuba, Japan. Since 2019 he has been with Institute of Materials and Systems for Sustainability (IMaSS), Nagoya University, Japan, where he is currently a Research Scientist in the Power Electronic Laboratory involved in wireless power transfer and application of new wide-band-gap semiconductor devices (SiC/GaN) for very high frequency converter to improve reliability, power density and efficiency.

Jun Imaoka (Member) received his M.S. and Ph.D. degrees in Electronic Function and System Engineering from Shimane University, Matsue, Japan, in 2013 and 2015, respectively. From October 2015 to March 2018, he worked at Kyushu University, Fukuoka, Japan as an Assistant Professor. From April 2018 to March 2021, he was an Assistant Professor at Nagoya University, Nagoya, Japan. He is currently an Associate Professor at the Institute of Materials and Systems for Sustainability (IMaSS), Nagoya University. His research interests include the design of integrated magnetic components, modeling for high-power-density power converters, thermal management for power converters, magnetic material application, and EMI of switching power supply.

Ryosuke Ishido (Non-member) received his B.E degrees in Kyoto Institute Technology, Kyoto, Japan in 2013 M.E degrees in Kyoto University, Kyoto, Japan in 2015. In 2018 he joined ROHM Co. Ltd., Kyoto, Japan. His research interests include gate drive circuit for wide-band-gap devices (SiC and GaN).

Yuta Okawauchi (Non-member) received his B.S and M.S. degrees in physics from Osaka City University, Osaka, Japan in 2008 and 2010, respectively. He is with the Research and Development Division, Rohm Company Ltd., Kyoto, Japan. His research interests include high power application.

Ken Nakahara (Non-member) received his B.S degree in physics from Kyoto University, Kyoto, Japan, in 1995, and the Ph.D. degree in chemical from Tohoku University, Sendai, Japan, in 2010. He is the Head of the Research and Development Center in ROHM Co. Ltd., Kyoto, Japan. His current research interests are widely ranged from power electronics, material science, and energy devices to artificial intelligence technologies.